Calibration of Weather Radars with a Target Simulator

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Abstract. We present findings from radar calibration experiments involving three radars operated by the Colorado State University (CSU) in the US and by the École Polytechnique Fédérale de Lausanne (EPFL) in Switzerland. The experiments were based on the comparison between measured radar variables and the known properties of artificial point targets electronically generated with a polarimetric radar target simulator (RTS) from Palindrome Remote Sensing. Radars under test included the
5   two magnetron-based radars CHILL and its mobile version SPLASH from CSU and EPFL's new solid state radar StXPol.

For the CHILL and SPLASH calibration measurements in Colorado, a mobile lifting platform was employed that elevated the target simulator instrument to approximately 15 m above ground. The creation of virtual targets with polarimetric signatures allowed for a direct calibration of polarimetric variables. While the SPLASH radar exhibited good Z_{dr} and sufficient Z_h accuracy, a remarkable precision and stability was found in CHILL's reflectivity data time series, where the reflectivity bias
10   compared to the virtual target was less than 0.2 dB over a one-hour time series.

Calibration issues that arise with solid state radar systems were investigated with experiments conducted with EPFL StXPol radar. This pulse compression system transmits a linear frequency-modulated long pulse as well as a non-modulated short pulse for observations at close ranges. The two pulses are separated in frequency by 50 MHz and consequently calibration targets were generated independently for the two channels. An excellent stability and accuracy was found for Z_{dr} in both channels.
15   While Z_h stability was also very high, a large reflectivity bias in both the long and the short pulse channel was detected.

For the first time, the article introduces and analyses a weather radar calibration procedure that is based on electronically generated radar targets. Experimental data suggests that precise absolute and differential calibrations can be achieved if data is obtained in an environment free from multi-paths and if the generated targets are precisely located in the center of the radar's range gate. Experimental shortcomings associated with limited sampling resolution of the radar scan over the targets are also
20   investigated.

1 Introduction

Advancements in meteorological radar technology have broadened the applicability of weather radar data to a wealth of complex applications such as high-resolution nowcasting of precipitation, lightning or hazardous winds, combined rain gauge / weather radar quantitative precipitation estimation, hydrological runoff forecasts, radar data assimilation in numerical weather prediction models and radar climatology. Therefore, the quality of weather radar data is critically important for weather services that provide advanced radar-derived meteorological and hydrological products to users. Not only advanced weather radar applications require highly accurate radar data: tasks like radar data exchange among national networks and the subsequent generation of radar mosaic products relies on radar data that are calibrated to the highest standards.

Focusing on the radar reflectivity, weather radar calibration involves all aspects of relating the received power that is backscattered by hydrometeors to the physical abundance and the location of the hydrometeors. To be able to completely interpret the captured radar data, the full path must be characterized: from pulse generation to transmission, propagation, backscattering, reception and digitalization (end-to-end calibration). In particular, the basis for the correct interpretation of the received radar signal is its amplitude relative to the transmitted signal. The ratio between the transmitted and the received power can be determined by explicitly measuring powers, gains and losses along the transmit and receive path. However, this is insufficient for advanced weather radar products that are based on dual-polarization measurements (Chandrasekar et al., 2015).

In this article, we present a dual-polarization radar target simulator (RTS) which is capable of generating electronic point targets with well-defined radar cross section (RCS) and Doppler properties. These known artificial targets serve as a reference for the complete end-to-end calibration of a polarimetric weather radar.

Up to now, standard techniques for radar reflectivity calibration with point targets employed external targets with known scattering properties, such as metal spheres and corner reflectors (Scarchilli et al., 1995; Joe and Smith Jr., 2001; Atlas, 2002). These metal spheres can be attached to balloons or drones (Bechini et al., 2010; Williams, 2013; van den Heuvel et al., 2018), facilitating this calibration technique. In Yin et al. (2019); Joshil and Chandrasekar (2022) and Ye et al. (2024) drone-based calibration processes are described in detail. The position of the sphere can be determined with a GPS sensor that is attached to the sphere. If a lifting platform is used, the rope lifting the calibration target must be sufficiently long so that the lifting platform does not contribute to the RCS.

Thanks to the relatively large beam width in the azimuth and elevation directions, trihedral corner reflectors have also been widely used for radar calibration purposes, mostly in Synthetic Aperture Radar (SAR) and other space-based radar applications (Gray et al., 1990). A major source of error in ground-based configurations is the scattering contribution from the ground itself. For weather radar calibration, previous studies have attempted to limit ground reflections using corner reflectors mounted on high wooden poles (Martner et al., 2003) or on a tripod that was installed on a mountain ridge (Schneebeli et al., 2013).

The expected accuracy of these standard methodologies is of the order of 1 dB, mostly accounting for the uncertainties in the antenna pointing and the target location within the radar's pulse volume. In fact, the radar's matched filter transforms the incoming rectangular pulse shape that is reflected from the point target into a triangular power distribution that is spread over several range gates. If the point target is not exactly located in the center of the range gate, the theoretical radar reflectivity that

is calculated from the target's RCS is higher than what is measured. The error caused by this uncertainty can be up to 6 dB in cases where the target has been placed exactly at the edge of a range gate.

The use of electronically generated targets offers several advantages, including greater control over target properties, improved precision, and the ability to eliminate positioning uncertainties. Their main advantage over static targets like metal spheres or corner reflectors is given by the fact that target properties can be changed, such that calibrations can be made at different ranges, velocities and radar cross sections, which enables calibration measurements over the whole dynamic range of the radar receiver, as shown in Schneebeli et al. (2023a). Target simulators were employed for weather radar calibration purposes during site acceptance tests of the third generation Swiss radar network Gabella et al. (2013); Germann et al. (2022) as well as during field campaigns, see e.g., Gehring et al. (2021).

This study explores the advantages [=] ng an RTS for the calibration of weather radars, ensuring accurate measurements of reflectivity, differential reflectivity, and Doppler velocity. This article is organized in a way to provide a systematic approach to radar calibration with RTS. Section 2 introduces the fundamental principles of weather radar calibration, discussing the importance of accurately interpreting backscattered signals from hydrometeors. Section 3 describes the operational aspects of the RTS, detailing how electronically generated targets provide a controlled and repeatable reference for calibration. The different radars under test are briefly presented in Section 4. The methodology employed in the calibration experiments is outlined in Section 5, highlighting the procedures for evaluating absolute reflectivity, differential reflectivity, and Doppler velocity accuracy. Finally, results from three distinct experiments, conducted on three different X-band weather radars, are presented in Section 6. As discussed in Section 7, the findings demonstrate the effectiveness of the RTS in identifying and correcting biases inherent to each radar system while also confirming the high temporal stability of measurements.

2 Electronically generated targets

An RTS is a system designed to create a simulated radar target at a specified range, incorporating a predefined Doppler shift and radar cross section (RCS). In the case of a monostatic radar, the RTS captures the transmitted radar pulses, modifies them, and retransmits them with a time delay corresponding to the intended target distance on the radar display. This time delay Δt (s) is given by

$$\Delta t = \frac{2\,(r_t - r_s)}{c}\,, \tag{1}$$

where r_t (m) represents the distance from the radar to the virtual target, and r_s (m) denotes the distance between the radar and the RTS.

To simulate a Doppler shift, the frequency shift f_D (Hz) applied to the reflected pulse is determined by [=]

$$f_D = \frac{2\,v}{\lambda}\,, \tag{2}$$

where v (m/s) represents the intended radial velocity of the simulated target, and λ (m) denotes the wavelength of the radar's carrier frequency.

Regarding the RCS, let p_r^{RTS} (W) denote the power of the radar pulse that is intercepted by the RTS. The power that is re-emitted by the RTS, p_t^{RTS} (W), is determined by the desired RCS, σ_b (m^2). In particular, following Schneebeli et al. (2023a) the fraction

90 $$K = \frac{p_t^{\mathrm{RTS}}}{p_r^{\mathrm{RTS}}} \tag{3}$$

between the powers transmitted and the received by the RTS is related to σ_b as

$$K = \frac{4\pi r_s^4 \sigma_b}{G_{\mathrm{RTS}}^2 \lambda^2 r_t^4} \, , \tag{4}$$

where G_{RTS} (-) represents the RTS antenna gain under the assumption that the gain of the RTS transmit and receive antenna are equal. The RTS setup that is used for the experiments presented in this article uses the same antenna for reception and

95 transmission, hence ~~the~~ assumption ~~certainly holds~~. Inside the RTS, the incoming digital samples are scaled by an amplitude multiplication factor k at the voltage level, i.e. $k^2 = K$, and thus

$$k = \frac{2\sqrt{\pi \sigma_b} r_s^2}{G_{\mathrm{RTS}} \lambda r_t^2} \, . \tag{5}$$

If the power fraction K is accurately controlled, a target with an RCS σ_b can be generated, making it suitable as a calibration reference. However, in weather radar applications, the priority is to provide a reference target with a specific radar reflectivity.

100 This requires generating a target with a defined RCS per unit volume, which in turn depends on the radar's pulse volume $\Delta V_p \tilde{\ }(\mathrm{m}^3)$,. Assuming a Gaussian-shaped radar beam, ΔV_p can be expressed as (Probert-Jones, 1962)

$$\Delta V_p = \frac{\pi \Theta^2 \Delta r \, r_t^2}{\ln(2) \, 8} \, , \tag{6}$$

with the half-power beam width of the radar antenna, $\Theta \tilde{\ }(\mathrm{radians})$, and the range extension of the pulse volume, Δr (m). Instead of applying the ~~latter~~ approximation for the pulse volume, which may lead to errors as high as 0.5 dB, it is more accurate to

105 calculate the pulse volume from the normalized antenna pattern $f(\theta, \phi)$ using

$$\Delta V_p = \int f^2 (\theta, \phi) \, d\Omega \, \Delta r \, r^2 \, , \tag{7}$$

with elevation angle θ, azimuth angle ϕ and solid angle differential $d\Omega \equiv \sin\theta \, d\theta \, d\phi$ (steradian).

Following standard weather radar textbooks (e.g. Rinehart, 1997), the relation between the effective radar reflectivity Z (mm^6/m^3) and σ_b is written as

110 $$\sigma_b = \frac{Z \pi^5 |\mathcal{K}|^2 \Delta V_p}{\lambda^4} \, , \tag{8}$$

where $|\mathcal{K}|^2 = 0.93$ is a parameter associated with the complex refractive index of liquid water. Combining eqs. (4), (6) and (8), the RTS power fraction K can be expressed as a function of the radar pulse width τ_{pw} (s), namely

$$\tau_{\mathrm{pw}} = 2\Delta r / c \, , \tag{9}$$

along with the range variables r_s and r_t, the RTS antenna gain G_{RTS}, the beamwidth Θ and wavelength λ of the radar under

115 test. Some of these variables can be precisely configured in the RTS, such as the r_s and r_t, while others, like G_{RTS}, must be known beforehand. Additionally, the parameters Θ and λ can be determined using the RTS itself. The radar wavelength is normally well-known before any measurements and does not need to be measured separately using the RTS. On the other hand, τ_{pw} and Θ are important to verify for the amplitude calibration of radar reflectivity using a target simulator. If the Gaussian beam approximation is not used, then the entire antenna pattern must be considered to compute the pulse volume as given in

120 eq. (7).

While measuring τ_{pw} is generally straightforward, as discussed in Section 5.2, determining the radar's Θ presents more challenges. The easiest approach is to use manufacturer-provided data. However, if these data are unavailable or unreliable, Θ must be determined separately through dedicated box scans around the generated target. Since simulated radar targets are point targets, their shape directly reflects the main beam pattern of the radar, making it possible to derive Θ, as demonstrated

125 in Schneebeli et al. (2023a). It was found that the standard deviation of $\sigma_{\Theta} = 0.02°$ inherent in successive measurements of Θ results in a reflectivity error of approximately $0.14\,\mathrm{dB}$.

With reference to the computation of K according to eq. (3), note that it is common that the predefined reflectivity of the calibration target often needs to be slightly adjusted a posteriori in case the analysis of the obtained pulse and radar data shows that the radars' real pulse width differs from the nominal one, or if other settings were not fully correct during the experiment.

130 The relevant parameter that is controlled by the RTS is always K and the corresponding reflectivity can be corrected if necessary during the analysis of the data. For instance, such corrections need to be applied if the distance r_s or the pulse width τ_{pw} differ from the RTS settings during the calibration experiment.

For system calibration, the relevant polarimetric radar variables are found in the direction where reflectivity reaches its peak. This direction can be identified by directly locating the maximum reflectivity in the radar data or by applying a Gaussian fit to

135 the data beforehand. A statistically robust calibration is then achieved through a series of repeated sector scans.

To calibrate the radar reflectivity Z using a point target, it is crucial to ensure the target is accurately positioned at the center of the range gate. A point target, when detected using a perfectly rectangular pulse, produces a parabolic response curve after matched filtering, similar to a triangular response in the voltage domain with a base width twice the pulse width. Since the radar's range resolution corresponds to the pulse width, there is a high probability that a point target will be sampled away

140 from its peak response. This issue is mitigated by adjusting the target's range while maintaining its radar reflectivity.

This matched filter effect is illustrated in fig. 1 where data from the StXPol radar (see section 4) has been used. A static target was generated at various distances from the radar while its reflectivity was kept constant at all positions. The target's normalized amplitude in the voltage domain as detected by the radar is plotted as a function of the target range. By applying a triangular least-square fitting procedure on the measured data and evaluating the width of the fitted triangle at half of its maximum, the

145 width of the matched filter can be experimentally inferred. In the data depicted in fig. 1, this width was determined to a value of $156.8\,\mathrm{m}$, which is very close to the nominal range gate size of $150\,\mathrm{m}$ corresponding to the employed pulse width of $\tau_{\mathrm{pw}} = 1\,\mu\mathrm{s}$.
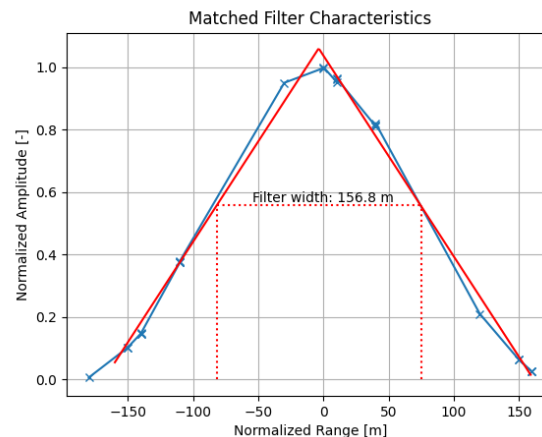
Figure 1. Matched filter characteristics inferred from a constant reflectivity target that was moved in range.

3 Radar target simulator

Palindrome p2q is a dual-polarization RTS developed for weather radar calibration purposes. Its capabilities for calibrating and monitoring weather radars are described in Schneebeli et al. (2023a) and a photo of the instrument is provided in fig. 2.

150 A basic description of the instrument together with an insight into its capability for measuring polarimetric phase differences is given in Schvartzman et al. (2024). The RTS receives radar pulses by either a polarimetric quad-ridged horn antenna with a gain 13.8 dB (employed for the experiments in Colorado) or by two orthogonally aligned standard gain horns with a gain of 19.5 dB (employed for the experiments in Lausanne) and performs analog down-conversion over two frequency stages before IQ signal components are digitized and sampled at a rate of up to 100 MHz per channel. For the experiments described in this

155 article, samples were acquired at a rate of 25 MHz. The digital radar pulses can be stored, modulated, and retransmitted with a given time delay while maintaining a pre-defined ratio between incoming and outgoing amplitudes. This enables polarimetric calibration targets with arbitrary reflectivity and Doppler characteristics to be generated.

In addition to weather radar calibration applications, the instrument has been employed for various radar testing tasks such as the calibration and commissioning of a multistatic C-band drone detection radar (Schneebeli et al., 2020, 2021, 2023b) as

160 well as for the generation of radar signatures of wind turbines (Schneebeli and Leuenberger, 2021).

Precise alignment of the RTS antenna towards the radar under test is crucial for accurate calibration measurements since the gain of the RTS antenna is known only in boresight direction. Correct pointing of the RTS antenna is ensured with an automated alignment algorithm: Once the RTS is setup at its location, the radar under test points toward the RTS and starts to transmit in staring mode. The RTS antenna is mounted on a precision tracker which is capable of performing high-resolution

165 box scans around the direction of the radar. Radar pulse power measurements that are acquired during the scanning procedure of the RTS antenna together with azimuth and elevation data of the RTS tracker lead to a Gaussian power distribution as a

Figure 2. Close-up view of the RTS.

function of the tracker coordinates. With a 2D Gaussian fitting procedure the direction of the power maximum is determined in a straightforward manner. This direction then serves as the correct pointing direction from the RTS towards the radar.

The RTS antenna is connected to the calibration units with RF cables. Since the signal path between the two is not calibrated during the operation of the RTS, it is important that high-performance cables are used, which maintain their pre-determined loss when the antenna is moved during the alignment procedure. The cable quality is even more important when the focus of the measurements is put on phase measurements, such as the experiment described in Schvartzman et al. (2024). To ensure phase and amplitude stability inside the RTS, all the critical analog parts like local oscillators, amplifiers as well as the whole calibration unit are thermally stabilized at a temperature of $38°C$ with an accuracy of $0.2°C$.

Figure 3 gives a schematic overview of the signal paths in the RTS. The labels and symbols used in this figure are described in table 1.

The purpose of the RTS is to retransmit the received signal in such a way that the power of the transmitted signal maintains a well-defined ratio to the power of the received signal. This ratio is referred to as the RTS factor K, which is defined in eq. (3) . The RTS software automatically calculates the power fraction K based on the predefined radar reflectivity (i.e. the desired

Table 1. Description and definition of the symbols shown in Figure 3.

Symbol	Description
Ref	Reference point where the ratio of the transmitted signal power p_t to the received power p_r must be equal to the factor K.
C	Circulator
S	Switch with two states. In *normal mode*, the signals from/to the circulator are bypassed to the reference point. In *calibration mode* the signals are bypassed to the calibration loop.
LB	Loop-back. In calibration mode, the transmit signal is looped back to the receiver.
Cal unit	Calibration unit, consisting of the circulator (C), the switch (S) and the loop-back (LB).
TX proc.	Transmit signal processing including digital-to-analogue (DA) conversion, signal conditioning and frequency up-conversion.
RX proc.	Receive signal processing including analogue-to-digital (AD), signal conditioning and down-conversion to base band.
p_r (W)	Received power at the reference point (Ref).
p_t (W)	Transmit power at the reference point (Ref).
K (-)	RTS factor. Ratio between the transmit power p_t to the receive power p_r at the reference point (Ref), see eq. (3).
p_{rd} (arbitrary digital units, adu)	Digital received power.
p_{td} (adu)	Digital transmit power.
K_d (-)	Digital RTS factor. Ratio between the digital transmit power p_{td} to the digital receive power p_{rd}, see eq. (10).
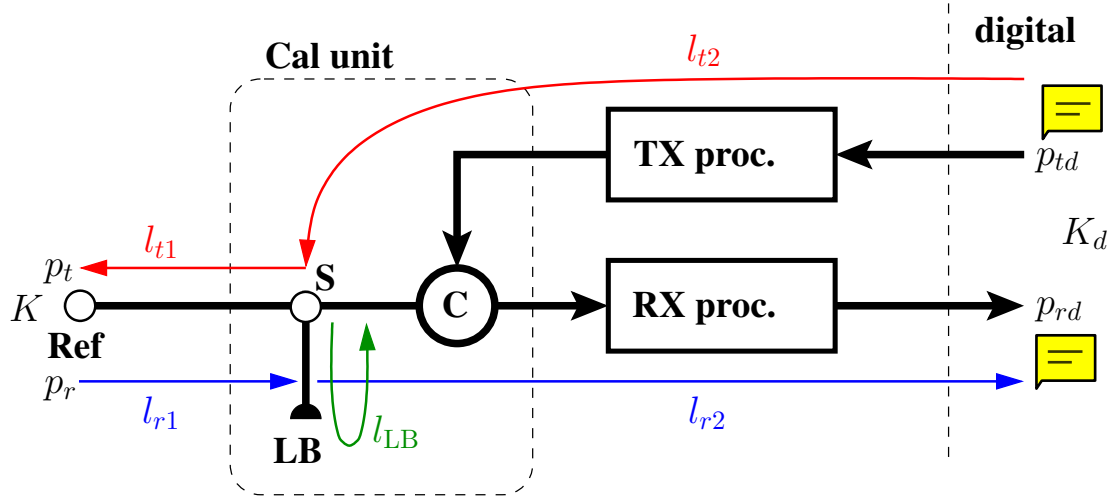
Figure 3. Schematic overview of the RTS signal paths. The description of the symbols is given in Table 1.

cross-section of the simulated target) and the desired distance of the calibration target, the distance between the radar and the RTS, the radar's pulse width and its half power beam width.

The calibration of the RTS is divided into two processes: static and dynamic calibration. The static calibration, which is done once (or every few months) in the laboratory before the RTS is used in operation, compensates for the frequency-dependent losses between the calibration unit and the antenna, as well as the losses of the calibration loop-back. The dynamic calibration, on the other hand, is performed periodically during operation, usually every minute, and compensates for mainly temperature-induced variations of the gains and losses in the receive and transmit paths.

3.1 Operational Mode

The digital loop-back factor K_d is the ratio of the digital transmit p_{td} to the digital receive power p_{rd} namely

$$K_d \equiv \frac{p_{td}}{p_{rd}} \ . \tag{10}$$

This factor is controlled by the RTS software and adjusted after the calibration loop. In the receive path, the digital receive power p_{rd} can is calculated as

$$p_{rd} = p_r \, G_{r1} \, G_{r2} \ , \tag{11}$$

where G_{r1} is the gain of the receive path between the reference point (Ref) and the switch (S), and G_{r2} is the gain of the receive path between the switch (S) and the received digital signal. The transmit power p_t is computed like

$$p_t = p_{td} \, G_{t2} \, G_{t1} \ , \tag{12}$$

where G_{t1} and G_{t2} are the gains of the transmit path between the switch (S) and the reference point (Ref), and between the transmitted digital signal and the switch (S), respectively. Combining the eq. (3), 11, 10 and 12, the digital loop-back factor

can be written as

$$K_d = \frac{K}{G_{r1}\, G_{r2}\, G_{t2}\, G_{t1}} \;.$$

(13)

3.2 Dynamic Calibration

During the calibration loop, a digital signal with power $p_{td,\mathrm{cal}}$ is generated in the field-programmable gate array (FPGA). It is reflected as an analogue signal within the calibration unit, guided back into the receive path and received again as a digital signal in the FPGA, denoted as $p_{rd,\mathrm{cal}}$. The received power is calculated as

$$p_{rd,\mathrm{cal}} = p_{td,\mathrm{cal}}\, G_{t2}\, G_{\mathrm{LB}}\, G_{r2} \;,$$

(14)

where G_{LB} is the gain of the loop-back path from the switch (S) to the loop-back (LB) and back to the switch (S). The ratio between the transmitted calibration power $p_{td,\mathrm{cal}}$ and the received calibration power $p_{rd,\mathrm{cal}}$ is the calibration constant K_{cal}.

$$K_{\mathrm{cal}} \equiv \frac{p_{td,\mathrm{cal}}}{p_{rd,\mathrm{cal}}} = \frac{1}{G_{t2}\, G_{\mathrm{LB}}\, G_{r2}} \;.$$

(15)

By using eq. (13) to replace the term $G_{r2}\, G_{t2}$, the digital RTS factor K_d becomes

$$K_d = K\, K_{\mathrm{cal}}\, \frac{G_{\mathrm{LB}}}{G_{r1}\, G_{t1}} \;.$$

(16)

3.3 Static Calibration

The last term in eq. (16) is assumed to be constant and must be measured before the instrument is used operationally:

$$K_{\mathrm{static}} \equiv \frac{G_{\mathrm{LB}}}{G_{r1}\, G_{t1}} \;.$$

(17)

Considering both the static and dynamic configurations, the digital RTS factor is calculated as

$$K_d = K\, K_{\mathrm{cal}}\, K_{\mathrm{static}} \;.$$

(18)

3.4 Determination of the Static Calibration Constant

The static calibration factor K_{static} can be determined by performing three measurements directly at the calibration unit. The first measurement is the gain of the receive path,

$$A_r \equiv \frac{p_{rd}}{p_r} = G_{r1}\, G_{r2} \;,$$

(19)

where the second equality follows from eq. (11). The second measurement is the gain of the transmit path

$$A_t = \frac{p_t}{p_{td}} = G_{t2}\, G_{t1} \;,$$

(20)

where we used eq. (12). The third measurement is the gain of the loop-back path

$$A_{\mathrm{LB}} \equiv \frac{p_{rd,\mathrm{cal}}}{p_{td,\mathrm{cal}}} = G_{t2}\, G_{\mathrm{LB}}\, G_{r2} \;,$$

(21)

see eq. (14). The static calibration factor K_{static} can then be calculated as

$$K_{\text{static}} = \frac{G_{\text{LB}}}{G_{r1}\,G_{t1}} = \frac{A_{\text{LB}}}{A_r\,A_t}\,. \tag{22}$$

225   The precise determination of K_{static} in the laboratory requires conducting the three distinct measurements outlined earlier, which necessitate the use of accurate RF measurement equipment. In our case, measurements were carried out using a signal generator capable of producing pulses with a wide range of amplitudes, along with a low-noise signal analyzer to detect weak pulses. If either the signal generator or the signal analyzer has calibration offsets, it is essential to compensate for these offsets dynamically throughout the measurement process. Furthermore, the measurement equipment must be synchronized to 230   a common frequency reference. Cable losses and reflection coefficients (S_{11} parameters) at the connection interfaces must also be considered to achieve measurement accuracies within 0.5 dB. As an alternative to using a signal generator and signal analyzer, K_{static} could also be determined with a Vector Network Analyzer (VNA) capable of operating with pulsed signals.

4 Radars

Table 2. Specifications of the three radars used in the present study.

Parameter	StXpol	CHILL	SPLASH
Radar frequency short pulse	9.385 GHz	9.41 GHz	
Radar frequency long pulse	9.335 GHz	-	
Polarization	dual (horizontal and vertical; STAR mode)		
Transmit power (per channel)	600 W	8kW	
Antenna gain	41.7 dB	43 dB	53 dB
Half power beam width	1.27°	0.3°	1.35°
Pulse width short	0.5 μs, 1.0 μs	0.5 μs	
Pulse width long	7.5 μs	-	
Long pulse modulation	linear	-	
Modulation bandwidth	2 MHz	-	
PRI	0.3 ms	1 ms	
Range step	75 m, 150 m	60 m	

4.1 CHILL

235 The CSU CHILL radar is an S- and X-band system that has been thoroughly described in the literature (e.g., Bringi et al., 2011; Junyent et al., 2015). In the described experiment, only CHILL's X-band system has been used, which consists of a magnetron transmitter and a polarimetric receiver that are mounted on a Gregorian dual-offset antenna with gain of 53 dB. The radar's main characteristics are provided in table 2.

4.2 SPLASH

240 The CSU SPLASH radar is a dual-polarization Doppler weather radar designed for dense network deployments. It is similar to RXM-25 which is described in Galvez et al. (2013). Operating at X-band, it covers up to 50 km with range resolutions below 40 m and simultaneously transmits and receives horizontal and vertical polarizations.

The radar uses a low-cost magnetron transmitter delivering 12 W per polarization channel with a peak power output of 8 kW. A dedicated signal path and digital frequency tracking system adjust the receiver settings in real time. Its analogue parallel
245 receiver includes low-noise amplifiers, a GPS-disciplined reference oscillator, and a high excess noise ratio (ENR) noise source for internal calibration. The digital receiver provides digitized I/Q signals and radar metadata over a 1 GB Ethernet link.

All signal processing and radar control run on a single server, handling real-time spectral processing, Doppler velocity unfolding, clutter filtering, and attenuation correction. The system supports both manual GUI-based and automated command-line operation, with automatic data transfer capabilities. All electronics are housed in enclosures that can be pressurized,
250 allowing operation in harsh conditions without a radome. More detailed radar characteristics are given in table 2.

4.3 StXpol

The Solid State X-band scanning Polarimetric radar (StXPol) built by ProSensing Inc. for EPFL is a radar system intended to provide measurements of clouds and precipitation and specifically designed to sustain high wind conditions and harsh cold environments in mountainous and polar regions. Able to operate in STAR (Simultaneous Transmission and Reception) or
255 alternate modes, it was employed in these tests in the former setting. It is equipped with a 1.82 m antenna (41.7 dB gain) and two 630 W solid-state amplifiers. The other radar main characteristics are provided in table 2.

5 Experiments

Calibration experiments with the three radars were conducted at two locations. SPLASH and CHILL were tested at the CHILL radar facility in Greely, Colorado, whereas StXPol was tested at the EPFL campus in Lausanne, Switzerland. For the exper-
260 iments in Colorado, fig. 4 shows how the RTS was lifted to a height of approximately 15 m with an elevated platform. The distance of the RTS to the SPLASH and CHILL radar was 470 m. The experiments with the SPLASH and CHILL radar were conducted in September 2023. For the experiment on the EPFL campus, the RTS was deployed from the roof of a building that was located at a distance of 356.7 m from the radar. Experiments with StXPol were conducted during ~~one~~ day in November

Figure 4. Left: Target simulator on the elevated platform with CHILL and SPLASH in the background. Right: Experimental setup in Lausanne.

2023 and repeated on ~~one~~ day in April 2024. Repetition was necessary to prove that reflectivity discrepancies between the short and the long pulse channel can be associated to the non-centered placement of the calibration target within the range gate.

5.1 Scan strategy and data acquisition

The sketch of the radars scan strategy is shown in Fig. 5 for the StXpol and Splash radars. The scan consisted of 25 subsequent sector scans that were spaced in elevation by $\delta\theta = 0.2°$ for SPLASH and StXPol and $\delta\theta = 0.1°$ for CHILL. The antenna speed was set to approximately $1°/s$, such that one full box scan was completed in slightly less than 5 minutes. The start elevation was $0°$.

Figure 5. Illustration of the box scan that is performed around the virtual target.

Box scan data was extracted at the range gate that exhibited the highest reflectivity. A 2D Gaussian fitting procedure was applied to the linear (i.e., non-logarithmic) reflectivity values of the box scan. The maximum of the fitted reflectivity is considered to be the relevant measured reflectivity that needs to be compared to the pre-defined target reflectivity. For other polarimetric or Doppler properties that need to be compared to the RTS values, a 2D Gaussian averaging kernel is constructed from the previously fitted reflectivity. If $\hat{Z}(\theta, \phi)$ designates the fitted reflectivity value when the radar points in the direction (θ, ϕ), the
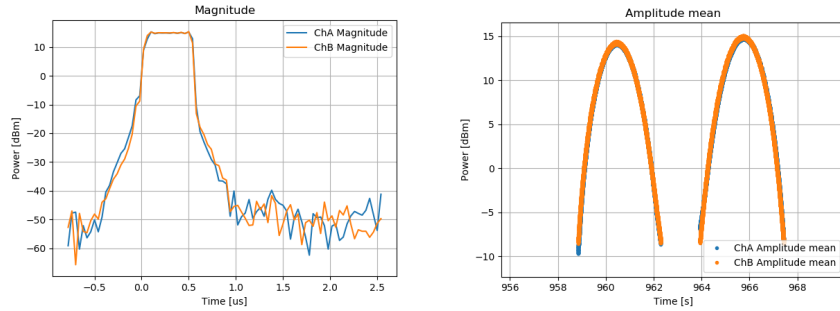
Figure 6. Left: Shape of the StXPol short pulse for both polarizations. Right: Pulse power maximum for both polarizations over two consecutive sector scans.

averaging kernel is defined as

$$L_{av}(\theta,\phi) = \frac{\hat{Z}(\theta,\phi)}{\sum_\theta \sum_\phi \hat{Z}(\theta,\phi)} \ . \tag{23}$$

Calling $B(\theta,\phi)$ the measured value of the polarimetric or Doppler observable of interest at the radar's pointing direction (θ,ϕ), we compute the following weighted estimate of the observable of interest:

280 $$b_{av} = \sum_\theta \sum_\phi L_{av}(\theta,\phi) B(\theta,\phi) \ . \tag{24}$$

With the CHILL radar, only 6 sector scans with a spacing of $0.1°$ in elevation were obtained for one repetition. Because of the size of the CHILL radar antenna, its far field is located at approximately 4.8 km, while the target simulator was set up at a distance to the radar of 470 m. In consequence, it is expected that the beam is not yet properly formed away from the center axis and therefore does not exhibit its final narrow shape yet. Nevertheless, it can be assumed that one sector scan hits the

285 RTS with sufficient accuracy. The subsequent analysis of the CHILL data is therefore based on only one sector scan that was performed at an elevation of $0.68°$.

5.2 StXPol Pulse measurements

5.2.1 Pulse power

During the StXPol experiments, the power of the radar pulses that were sampled with the RTS was continuously and accurately

290 determined in an absolute manner thanks to an update of the RTS firmware that allowed the comparison of incoming power with an internal reference pulse source. Although such absolute power measurements are unnecessary for reflectivity calibration tasks, where only the fraction between the incoming and outgoing RTS power is relevant, the additional quantitative data provide useful information on the radar performance as well as on potential multipath contamination. Some of the acquired StXPol pulse measurements are therefore detailed ~~in the following~~.

295 Fig. 6 shows the shape of the short pulse on the left panel and a series of maximum pulse power amplitudes over the suite of two sector scans on the right panel. An important and obvious feature of both figures is the fact that the data from the two RTS channels overlap very well. This not only indicates that the two radar channels transmit an equal amount of power, it is also a first confirmation that measurements are not affected by multi-path contamination because the two polarizations are unlikely to be equally affected by multi-path.

300 The two sector scans exhibit the RTS maximum receive power P_{rts} and hence it can be used to estimate the radar transmit power P_{rad} according to the Friis transmission equation (e.g., Ulaby and Long, 2014):

$$P_{\text{rad}} = \frac{P_{\text{rts}}}{G_{\text{rad}} G_{\text{rts}} \left(\frac{\lambda}{4\pi r_s}\right)^2} \, , \tag{25}$$

where $G_{\text{rad}} = 41.7$ dB and $G_{\text{rts}} = 19.5$ dB are the antenna gains of the radar and the RTS, respectively and $r_s = 356.7$ m is the the distance between the radar and the RTS. With $P_{\text{rts}} = 14.9$ dBm (determined from the maximum value of the right panel

305 of Fig. 6) a value of $P_{\text{rad}} = 472.34$ W is calculated, which corresponds to the transmit power of one polarization right behind the radar antenna. This value can be compared with the direct measurement made one day later with the spectrum analyzer at the waveguide that feeds the radar antenna. With the spectrum analyzer, a value of $P_{\text{rad}} = 501$ W was obtained ~~and hence a~~ difference of 0.25 dB between the two methods ~~is found~~. Since this difference is small, it is concluded that multi-path effects that might affect pulse amplitudes can be neglected.

310 ### 5.2.2 Pulse modulation
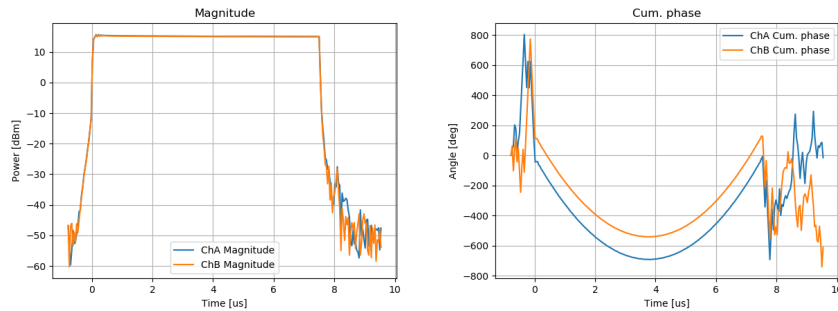
Figure 7. Left: Shape of the StXPol long pulse for both polarizations. Right: Cumulative phase over one long pulse duration for both polarizations.

The cumulative phase of a linear frequency modulated (LFM) chirp is supposed to exhibit a parabolic shape. The image given in the right panel of Fig. 7 depicts the measured cumulative phase of the radar's modulated long pulse with a nominal bandwidth of 2 MHz. The shown parabolic phase behavior $\Phi(t)$ can be described as

$$\Phi(t) = \left(t - \frac{\tau_{\text{pw}}}{2}\right)^2 \frac{4\Phi_{\text{tot}}}{\tau_{\text{pw}}^2} \, , \tag{26}$$

with pulse width τ_{pw} and total cumulative phase Φ_{tot}. The frequency hub f_{hub} is calculated from eq. (26) as

$$\frac{1}{2\pi}\left(\left.\frac{d\Phi(t)}{dt}\right|_{t=\tau_{\mathrm{pw}}} - \left.\frac{d\Phi(t)}{dt}\right|_{t=0}\right) = \frac{4\Phi_{\mathrm{tot}}}{\pi\tau_{\mathrm{pw}}} = f_{\mathrm{hub}} \tag{27}$$

This result together with the measurement of $\Phi_{\mathrm{tot}} = 652°$ (determined from the beginning and the minimum of the parabolic given in Fig. 7) leads to a modulation bandwidth of $f_{\mathrm{hub}} = 1.937$ MHz if a pulse width of $\tau_{\mathrm{pw}} = 7.4805$ μs is assumed. The determined value of the modulation bandwidth is close to the nominal value of 2 MHz. It is therefore assumed that the correct pulse compression ratios were applied to the reflectivity data provided by the radar.

6 Calibration Results

6.1 StXPol

Table 3. StXPol reflectivity calibration results

Parameter	Date	Pulse channel	Target size	Target range	Pulse length	K	bias	std
Z_h	11/23	long	39.5 dBZ	10.13 km	0.5 μs	$1.237\,10^{-5}$	5.5 dB	0.08 dB
Z_{dr}	11/23	short	0 dB	10.13 km	0.5 μs	-	0.06 dB	0.043 dB
Z_h	04/24	short	60 dBZ	7.9 km	1.0 μs	0.06337	4.9 dB	-
Z_{dr}	04/24	long	0 dB	7.9 km	1.0 μs	-	0.3 dB	0.04 dB
Z_{dr}	04/24	short	0 dB	7.9 km	1.0 μs	-	0.06 dB	0.013 dB

Since StXPol possesses two independent signal processing chains per polarization, i.e., one for the unmodulated short pulse (SP) and another for the frequency modulated long pulse (LP), calibration measurements were performed individually and sequentially for both channels with the different modulation schemes. A priori, it was not known that these two channels (SP and LP) exhibit a slight difference in range that might be induced by filtering effects. This range discrepancy requires that the placement of the generated target is individually adjusted for the two channels, in order to locate the target exactly at the range gate center, as shown in Fig. 1. This matched filter effect deteriorates the accuracy of the absolute calibration but in principle does not effect the calibration of the differential reflectivity, Z_{dr}.

Regarding the first experiment in November 2023, the target range was set to 10.13 km, which is optimized for the LP channel. Due to an error in the target simulator software, the transmit path amplifier settings of the RTS were beyond optimal in the LP measurement set-up, causing digital noise in the generated target and a reduced signal-to-noise ratio (SNR) in the corresponding radar data. This effect was manifested in the maximum values of the generated targets' co-polar correlation coefficients, ρ_{hv}: for SP a value of $\rho_{\mathrm{hv}}^{\mathrm{SP}} = 0.996$ was achieved while for LP a value of $\rho_{\mathrm{hv}}^{\mathrm{LP}} = 0.9984$ was found. The reduced SNR negatively impacted Z_{dr} much more than the absolute reflectivity, hence it was decided to only keep the LP measurements

from November 2023 for absolute reflectivity calibration. The SP measurements from November 2023 exhibited a slight range offset, but SNR was excellent and therefore these measurements were only used for differential reflectivity calibrations.

As to the tests conducted in April 2024, SNR was excellent for both LP and SP, but this time the LP measurements exhibited the range offset. Therefore, Z_{dr} could be calibrated for both pulse lengths and only SP data was considered for absolute reflectivity calibration.

Relevant StXPol calibration results for absolute and differential reflectivity are provided in Table 3. The RTS power fraction, K, is provided for absolute reflectivity calibrations only and not for differential reflectivity, where the absolute K value is irrelevant. In addition, the standard deviation of the time series of measurements is calculated only if more than three box scans per target were completed.

6.1.1 Reflectivity

An example of a box scan radar reflectivity acquisition performed around an electronic target that was generated for the short pulse channel is shown in Fig. 8. The target intensity was set to 60 dB. The maximum of the Gaussian fit (red contour lines in Fig. 8) assumed a value of 55.1 dB and hence a large reflectivity bias can be diagnosed.
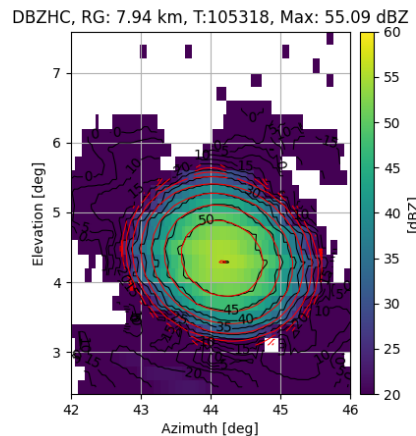
Figure 8. Reflectivity data obtained from a box scan around the virtual target that was generated at a distance of 7.86 km with a reflectivity of 60 dBZ.

A similar reflectivity bias was found in the November 2023 experiment in the long pulse channel, as seen in Fig. 9. For the time series shown, 7 box scan repetitions were performed around a target with a pre-defined reflectivity of 39.5 dBZ. The plotted data points correspond to the maximum of the Gaussian fit applied to the linear 2D reflectivity data. In this experiment, the target size has initially been set to 40 dBZ but was corrected afterwards since the radar-RTS distance was not set correctly during the experiment.

Direct comparisons between the short and the long pulse channel cannot be made, since it was found that a range offset of
355   40 m persists between the two channels. Since the target range was optimized for the long pulse channel in November 2023
and for the short pulse channel in April 2024, a calibration offset of approximately 2 dB between the two channels is found for
each of the two days, which is explained with the plot shown in Fig. 1.
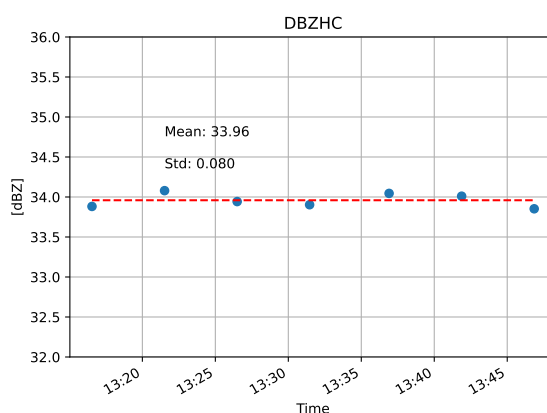
Figure 9. Reflectivity time series of a target with a size of 39.5 dBZ.

Despite these experimental shortcomings, the reflectivity bias remained consistent over the two experiments that were sepa-
rated by four months. In addition and as seen in Fig. 9, the short-term stability was high. The reflectivity standard deviation of
360   0.08 dBZ, determined from time series data during the November 2023 experiment, was found to be similar for the SP and LP
channel.

6.1.2   Differential Reflectivity

A box scan acquisition of the differential reflectivity is given in the left panel of Fig. 10, while the right panel provides the
corresponding time series. The data shown was acquired with the short pulse channel in November 2023, with the differential
365   reflectivity of the target ~~being~~ set to 0 dB.

The box scan plot exhibits a distinctive pattern that subdivides the Gaussian antenna pattern into 4 quarters. This pattern is
assumed to be induced by the four struts of the antenna that hold the feed in place. Similar patterns were observed with solar
box scans obtained with a C-band radar of the German weather service in Hohenpreissenberg (Frech and Hubbert, 2020), and
additional directional biases can be caused by radomes with non-random geometric patterns (Figueras i Ventura et al., 2021).
370   Since solar measurements are only passive, the magnitude of the antenna effect is smaller than for the active measurements
used in our case. It is noteworthy that a value of $Z_{\mathrm{dr}} = 0 \ \mathrm{dB}$ is achieved only in the main beam direction of the antenna. With
the averaging kernel method described in eqs. (23) and (24), the box plot data is weighted in order to obtain the individual data
point for the time-series given in the right panel of Fig. 10.
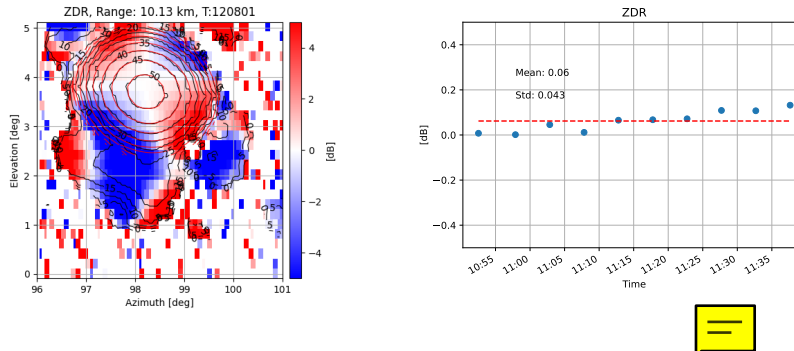
Figure 10. Left: Differential reflectivity pattern of a box scan acquired with the short pulse. Right: Time series of the differential reflectivity where the target Z_{dr} was set to 0 dB.
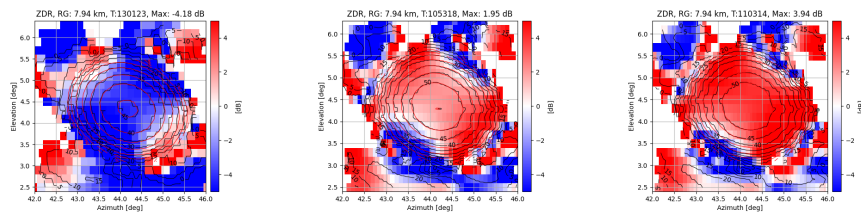
Figure 11. From left to right: Box scans of Z_{dr} around targets that were generated with differential reflectivity values of -4, 2 and 4 dB.

The low bias as well as the high short-term temporal stability suggest that the radar is well calibrated with respect to the
375 differential reflectivity. For the LP data, a similar data acquisition procedure exhibited a Z_{dr} bias of 0.5 dB.

Up to this point, and also for the subsequent analysis of the differential reflectivity calibration for SPLASH and CHILL,
the simplest case with a target exhibiting a differential reflectivity value of $Z_{\mathrm{dr}} = 0$ dB ~~has been~~ used. In principle, there
is no reason to believe that a dependence exists between the Z_{dr} value of the target and the respective calibration biases.
However, given ~~the influence~~ of polarization channel coupling on the Z_{dr} bias ~~as~~ investigated in many articles (e.g., Wang
380 and Chandrasekar, 2006; Zrnić et al., 2010), it seems meaningful to perform calibration measurements with Z_{dr} targets that
are different ~~to~~ 0 dB. To do so, three targets with Z_{dr} values of -4 dB, 2 dB and 4 dB were generated, where the targets with
the negative Z_{dr} exhibited a horizontal reflectivity of 60 dBZ, while the target with the negative Z_{dr} exhibited a horizontal
reflectivity of 50 dBZ. The data stems from the short pulse channel and was ~~acquired~~ in April 2024. The respective box scans
can be seen in fig. 11. The overall bias of these three ~~acquisitions~~ is -0.095 dB and hence a difference of 0.15 dB in the Z_{dr}
385 bias between the 0 dB targets and the non-zero dB targets can be ~~stated. From the authors' point of view~~, the number of scan
repetitions is ~~too low~~ and the variance in the targ... properties too high to draw more detailed conclusions than the statement
that no significant change in the Z_{dr} bias can be associated with a change of the target's Z_{dr}.
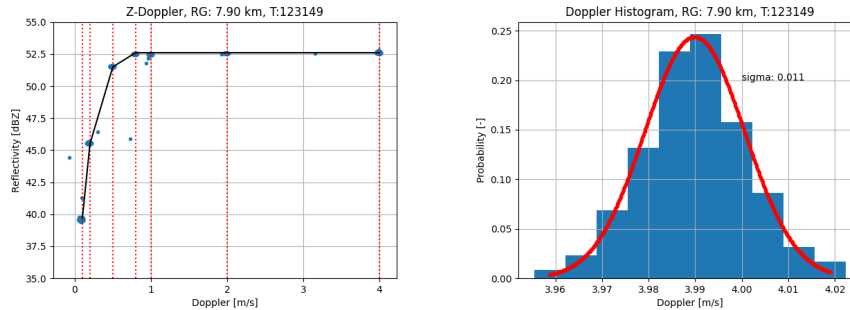
Figure 12. Left: Filter curve of a 0.83 m/s wide clutter filter that was tested with a stable reflectivity target with changing Doppler properties. The red lines indicate the Doppler speeds that were given to the target. Right: Histogram of the same data as shown in the panel on the left-hand side, but extracted around a Doppler speed of 4 m/s. Data was acquired in FFT mode.

6.1.3 Velocity

Doppler velocities can be attributed to electronically generated point targets in a very precise manner. Likewise, weather radars
390 are capable of measuring Doppler velocities very precisely. For instance, StXPol's velocity bias was found to be lower than 0.01 m/s. Velocity calibration is the ~~re~~ usually unnecessary. The advantage of using generated targets that exhibit specific Doppler properties is nevertheless manifold. Since the radar can be operated with a ~~Doppler~~ filter to further eliminate unwanted ground reflection ~~~~ meaningful to test the behavior of this filter, as demonstrated in the left panel of Fig. 12. The radar was operated in staring mode and pointed directly towards the RTS. While the generated target reflectivity remained constant, the
395 target speed was reduced from 4 m/s to 0.1 ms. The radar's Doppler filter was set to a width of 0.83 m/s. It is observed that the suppression of targets with velocities that are within the filter width is not very sharp. In addition to theoretical verification of filter behavior at the signal processing level, this technique - based on generated targets that can be tuned to specific Doppler properties - provides the only means of thoroughly testing the implementation of the radar's Doppler filter.

The Doppler time interval histogram can be determined from the same measurement by extracting data around a specific
400 Doppler velocity. For the histogram that is plotted in the right panel of Fig. 12, reflectivity data that originates from a 4 m/s Doppler target is used. We find a narrow Gaussian distribution with a width of 0.011 m/s. The non-zero spectrum width stems from phase noise contributions of the transmitter, the radar receiver as well as from the RTS phase noise. It is important to note that this histogram is not identical to the Doppler spectrum. The Doppler spectrum width was obtained with the radar during the scanning process and resulted in a value of 0.2 m/s for an antenna speed of $1°/\mathrm{s}$. While the histogram shows how
405 the mean of the Doppler spectra is distributed, one cannot infer one from the other. However, it shows that the spectral width that is inherent in the measurements is much wider than the fluctuations of the maxima and hence underlines that very precise Doppler measurements are obtained with the radar.

Fig. 13 finally shows the box scan acquisition of the co-polar correlation coefficient, ρ_{hv}, which offers a practical way to assess imperfections in beam matching and low channel isolation. Virtually-generated polarimetric radar targets as well as

410 low intensity stratiform rain are supposed to exhibit perfect correlation between the polarimetric channels. Values below 1 are caused by receiver noise and antenna performance, as stated in Mudukutore et al. (1995). Values as high as $\rho_{\mathrm{hv}} = 0.9995$ for the long pulse channel and $\rho_{\mathrm{hv}} = 0.9996$ for the short pulse channel were obtained, both with low standard deviations over time of the order of $\sigma_{\rho_{\mathrm{hv}}} \sim 10^{-5}$. The remarkably large and temporally stable nature of ρ_{hv} of a bright scatterer has been reported in Gabella (2018) and Gabella (2021) where it has been concluded that this quantity can be used for monitoring hardware deficits.
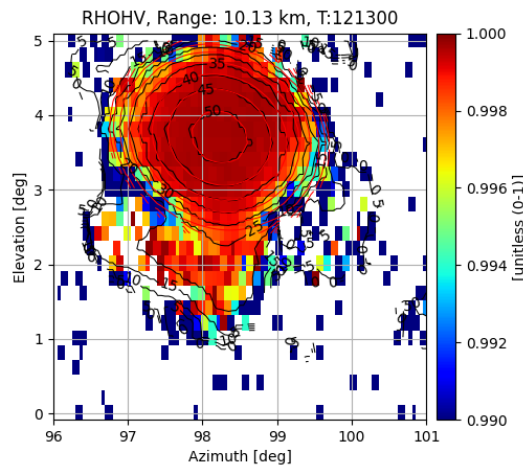
Figure 13. Radar measurements of the copolar correlation of the virtual target. Measurements acquired with the short pulse are shown.

6.2 CHILL

415

The RTS was set up at a distance of 470 m ~~to~~ the radar at a height of approximately 15 m above ground. A photo of the experimental setup is shown in the left panel of Fig. 4. In contrast to the box scan data acquisition that was performed for SPLASH and StXPol, relevant data was extracted from one of six sector scans that were made in the direction of the RTS. A vertical cut through the sector scans at the location of the generated target is shown in Fig. 14. CHILL's large antenna and its

420 narrow beam width of $0.3°$ ~~make possible~~ the identification of slight pointing errors. As seen in the right panel of Fig. 14, the reflectivity is slightly shifted away from the direction of the antenna movement due to a gear backlash of $0.15°$.

Similar to the procedure detailed for the StXpol radar, the target also had to be placed in the center of the range gate. As seen on the sector representation of the reflectivity data in the left panel of Fig. 14, the two range gates that are adjacent to the center range gate both exhibit similar reflectivity values, which indicates that the target was correctly placed in the range gate's

425 center.

For reflectivity calibration purposes, a target 40 dBZ target at a range of 18 km was generated. The initially chosen reflectivity value had to be corrected to 40.9 dBZ due to changes in the definition of the pulse volume. More specifically, the relevant RTS power fraction was set to a value of $K = 0.1370$. This value, together with the RTS antenna gain $G^{\mathrm{RTS}} = -6.36$ dB, the
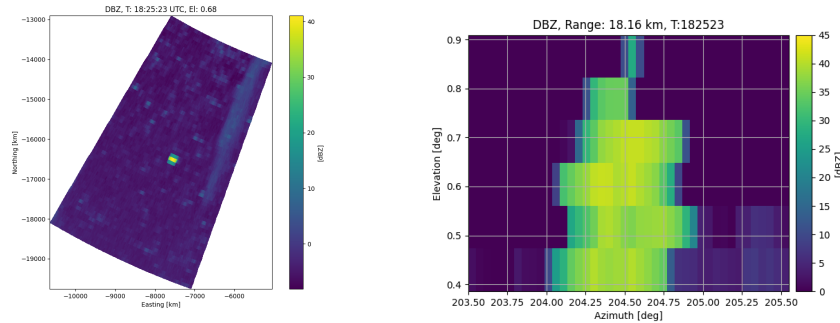
Figure 14. Left: CHILL radar reflectivity sector scan at the elevation of the RTS. Right: Vertical cut of CHILL reflectivity data through 6 sector scans extracted at the location of the generated target.

distances $r_s = 470$ m and $r_t = 18.01$ km and the pulse width $\tau_{\mathrm{pw}} = 0.5$ μs leads to the indicated reference reflectivity of the generated target. The reason that $G^{\mathrm{RTS}} = -6.36$ dB is so low is due to the fact that an additional 20 dB attenuator was placed between the antenna and the reference point *Ref* (see Fig. 3). This was done to protect the RTS from the strong radar power from CHILL, owing to the high antenna gain of 53 dB and the short distance between the RTS and the radar antenna. The value of the attenuator was accounted for in the RTS antenna gain with $G^{\mathrm{RTS}} = 13.64$ dB $- 20$ dB $= -6.36$ dB, with 13.64 dB being the antenna gain of the quad-ridge horn antenna at a frequency of $f = 9.41$ GHz, as determined in a calibration laboratory.

It is important to note that the RTS was set-up in the radar's near field. The far-field of the X-band CHILL radar starts at approximately 4.8 km, significantly beyond the radar-RTS distance of 470 m. However, it is not expected that this fact induces shortcomings for absolute reflectivity calibration measurements.

A one-hour reflectivity time series ~~was compiled~~ from sector scans that were performed at an elevation of $0.68°$. The radar's reflectivity data underwent a 1D Gaussian fitting procedure, after which the maxima of the fitted curves were used to ~~compile~~ the plot shown in Fig. 15. The extracted radar data (mean: 41.1 dBZ) exhibits a good agreement with predefined target reflectivity and the temporal stability is very high over one hour (standard deviation: 0.026 dB).

An overview of the reflectivity calibration results can be found in Table 4. Slightly less convincing are the results for the differential reflectivity, Z_{dr}. Although the stability over one hour was again very high, with a standard deviation in Z_{dr} as low as 0.037 dB, the bias of -1.43 dB in differential reflectivity is considerable. At the time of writing the origin of this bias has not been fully identified. An almost identical setup for the SPLASH calibration experiment, which was conducted just one day before the CHILL measurements, provided reasonable Z_{dr} calibration data. It is therefore assumed that the generated calibration target exhibited correct differential reflectivity properties. However, CHILL's extremely narrow antenna beam width of $0.3°$ makes the differential reflectivity calibration with a point target very demanding. The chosen scanning resolution in elevation of $0.1°$ is likely to be too low for accurate Z_{dr} calibration since the antenna beam center might have been missed by some hundredth of degrees. While the impact of this effect on the absolute reflectivity is low, it is considerable for Z_{dr} due to its high variation within the antenna beam. This can be illustrated by using the sector scan at an elevation of $0.78°$, i.e.,
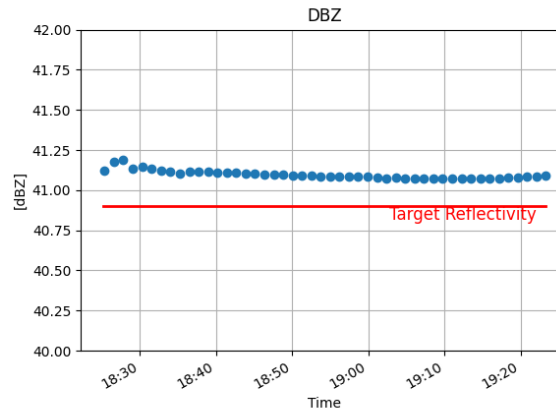
Figure 15. Time series of the maximum of a Gaussian fitted sector scan over a generated point target.

$0.1°$ above the scan that is used for the current analysis. By using this scan, the mean of the Z_{dr} time series calculates to a value of 4.2 dB. It is speculative to calculate a mean from this value and the Z_{dr} value from the sector scan below, but the large difference between the two values serves as an indication that for future experiments, a higher scan resolution would be appropriate for such a narrow antenna beam width.

6.3 SPLASH

An experiment similar to the one with the CHILL radar was conducted on September 13, 2023 with the SPLASH radar. This mobile radar is very similar to the X-band CHILL radar with the antenna being the main difference. SPLASH has been set-up close to CHILL such that the radar-RTS distance was $r_s = 431$ m. The target's radar reflectivity at horizontal polarization was initially set to $Z_h = 40$ dBZ, but had to be corrected in the analysis to $Z_h = 38.5$ dB. This was due to a correction of r_s and a difference between the measured and nominal values of the pulse width (0.41 μs and 0.5 μs respectively). The relevant RTS power ratio was set to $K = 6.638\,10^{-4}$. The half-power beam width Θ of the radar antenna was obtained from the 2D Gaussian fit of the reflectivity (as shown in Figure 16). By taking into account that Θ is inferred as the 6 dB beam width from the radar reflectivity, a value of $\Theta = 1.35°$ was obtained in this manner. Box scans around the generated target were performed similarly to those for the StXpol experiment.

The box scan of the reflectivity data shown in Fig. 16 exhibits some missing data at the upper left corner of the target. The reason for this feature is the internal calibration procedure of the RTS that was executed when the radar was pointing in this direction. As seen from the contour lines of the measured reflectivity data (black) and the contour lines of the Gaussian fit (red), the fitting procedure is only marginally affected by this effect. In fact, the reflectivity representation of the generated target exhibits a distinctive regular Gaussian behavior, which justifies the usage of this data for the determination of the half power beam width of the radar antenna. The maximum of the reflectivity fit was found at $Z_h^{\mathrm{max}} = 37.43$ dBZ, such that the

reflectivity bias was calculated to a value of 1.27 dB. A standard deviation of this value is not given in Tab. 4, since only two box scan repetitions with the same target properties were conducted.

Table 4. CSU radar calibration results

Parameter	Radar	Target size	Target range	Pulse length	K	bias	std
Reflectivity	SPLASH	38.7 dBZ	6.88 km	0.41 μs	$6.638 \cdot 10^{-4}$	1.27 dB	-
Z_{dr}	SPLASH	0 dB	6.88 km	0.41 μs	-	0.56 dB	-
Reflectivity	CHILL	40.9 dBZ	18.16 km	0.5 μs	0.1370	0.2 dB	0.026 dB
Z_{dr}	CHILL	0 dB	18.16 km	0.5 μs	-	-1.43 dB	0.037 dB

The value that is relevant for the calibration of the radar differential reflectivity, Z_{dr}, is extracted from the data shown in right panel of Fig. 16 with the above-mentioned averaging kernel method (see section 5.1). For a target with a nominal differential reflectivity of $Z_{dr} = 0$ dB, a differential reflectivity offset of 0.56 dB is found from the depicted box scan. An apparent difference in the differential reflectivity patterns between SPLASH and StXPOL can be noted. In order to fully explain the two patterns, a detailed investigation requiring measurements of co- and cross-polar antenna patterns would be necessary. With the data at hand, it is speculated that the two antennas exhibit different co- and cross-polar rad ⬜ patterns, with the cross-polar maximum located on the co-polar main lobe for the SPLASH antenna and four equal cross-polar maximum lobes arranged around the co-polar main lobe for the StXPOL antenna, as ~~sketched~~ in Zrnić et al. (2010). The four cross-polar maxima with alternating phases can explain the four distinct Z_{dr} features located at elevations of $3.75°$ and $5.75°$ and azimuth angles of $42.5°$ and $45.5°$ $5.75°$ in Figure 11. These features are absent in the right panel of Fig. 16, where a circular Z_{dr} minimum in the center of the radiation pattern is found instead.
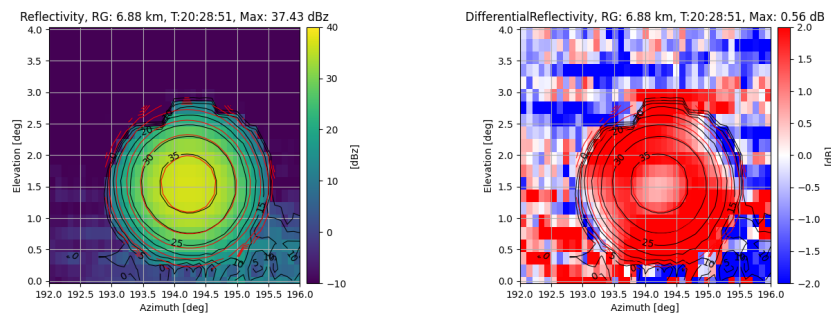
Figure 16. Reflectivity data obtained from a box scan around the virtual target that was generated at a distance of 6.88 km with a target reflectivity of 38.7 dBZ and a differential reflectivity of $Z_{dr} = 0$ dB.
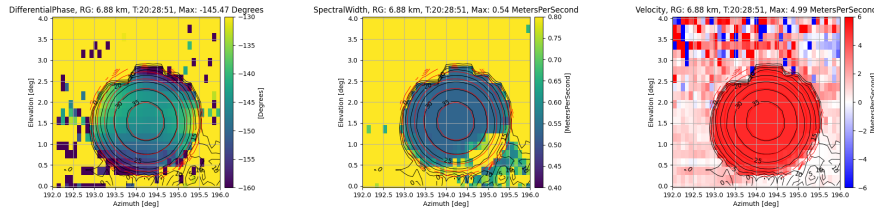
Figure 17. From left to right: Box scans of the differential phase Ψ_{dp}, the Doppler spectrum width $\sigma(v_D)$ and the Doppler velocity v_D from a target that was scanned with the SPLASH radar and exhibited a Doppler velocity of 4 m/s .

6.3.1 Phase-based measurements

Apart from the clutter filter testing section 6.1.3, the main focus of the measurements presented up to now has been on power-based radar observables. To present a complete view of the measurement capabilities of an RTS, fig. 17 depicts box scans of the radar's differential phase Ψ_{dp}, the Doppler spectrum width $\sigma(v_D)$ and the Doppler velocity v_D.

As expected, the v_D box scan exhibits a homogeneous pattern with a value at the center of the antenna that is very close to the Doppler velocity of the generated target. Towards the lower right corner of the box scan, where reflectivity contamination is increasing, velocities start to degrade from their nominal values. This effect is more prominent in the spectral width data. Ground clutter with spectral components around the zero Doppler line leads to a broadening of the overall spectrum and hence to the increase of $\sigma(v_D)$ in the lower right corner of the box scan.

The total differential phase Ψ_{dp} is shown in the first panel of ~~fig~~. 17. Neither the RTS nor the radar were corrected for differential phase offsets, hence only the relative differential phase distribution over the aperture is considered. Antenna differential phase patterns have been measured in Mudukutore et al. (1995); Hubbert et al. (2010); Moisseev et al. (2010); Myagkov et al. (2015), mainly for assessing the quality of dual-polarization measurements. In general, the authors state that high-quality antennas exhibit lower Ψ_{dp} variations over the aperture. Within the half-power beamwidth, Ψ_{dp} variations on the order of 2° were found for the SPLASH radar, which is qualitatively comparable to the findings in Moisseev et al. (2010) for two C-band radars. A more in-depth analysis of the Ψ_{dp} distribution is beyond the scope of this article. The respective data is shown solely to illustrate the antenna quality assessment capabilities of measurements based on generated targets.

7 Conclusions

The use of RTS for weather radar calibration offers several advantages, including high precision, repeatability, and flexibility in generating artificial targets with well-defined radar cross-sections (RCS) and Doppler properties. Unlike static calibration techniques that rely on physical targets such as metal spheres or corner reflectors, RTS ~~enable~~ the generation of point targets with controllable parameters, allowing for more robust calibration across a wide range of operational conditions. Additionally, RTS facilitate the evaluation of radar performance without the logistical challenges associated with deploying physical targets.

In evaluating the biases of different radar systems, our experiments highlight key differences in absolute and differential reflectivity calibration, as well as Doppler velocity accuracy. The CHILL radar demonstrates high stability in its reflectivity
510   measurements, with a minimal bias of approximately 0.2 dB over a one-hour time series, indicating excellent calibration performance. Calibration analysis revealed a reflectivity bias of roughly 1.27 dB in the SPLASH radar. Incorporating this adjustment into the data results in well-calibrated reflectivity measurements.

The StXPol radar, on the other hand, showed a significant reflectivity bias in both its long and short pulse channels, with deviations of 5.5 dB and 4.9 dB, respectively. This offset did not originate from target misplacement but rather from the radar
515   itself. Since the reflectivity bias was inherent in the short and in the long pulse, persisted over 6 months, was not induced from a target misplacement within the range gate and also cannot be explained with multi-path effects, we are confident that a radar mis-calibration is causing this significant discrepancy. Despite this bias, the StXPol radar exhibited high temporal stability, reinforcing confidence in its measurement consistency over time.

For differential reflectivity calibration, the CHILL radar exhibited a considerable bias of -1.43 dB, suggesting the need for
520   further investigation either into system-specific sources of error or into possible drawbacks of the experimental setup. In the interpretation of this measured bias it needs to be taken into account that X-band CHILL is a particularly difficult radar to calibrate due to its extremely narrow beam width of 0.3°. In elevation, the generated target was scanned with a resolution of 0.1°, which is most likely sufficient for absolute reflectivity calibration but probably insufficient for Z_{dr} calibration due to the large variation of this observable within the antenna beam. It is concluded that the scan resolution for accurate Z_{dr} calibrations
525   should be smaller than a tenth of the antenna's half power beam width.

The SPLASH radar displayed a Z_{dr} bias of 0.5 dB, which falls within an acceptable range but still warrants minor corrections for improved accuracy. The StXPol radar performed well in differential reflectivity calibration, with biases of the order of ± 0.06 dB for the short and 0.3 dB for the long pulse, indicating high precision in polarimetric measurements.

The RTS also allows one to test the effectiveness of clutter filters by varying the speed of the generated target, making it
530   possible to evaluate the filter response across different Doppler velocities.

A critical factor in achieving accurate reflectivity calibration is the precise placement of the RTS-generated target within the center of the radar's range gate. If the target is positioned at the edge of the range gate, the measured reflectivity can be significantly lower than the expected value, introducing biases as large as 6 dB. Proper target placement is essential to ensuring measurement accuracy across different radar systems.

535   Additionally, the need for a multipath-free setup is crucial for accurate calibration results. Multipath effects can lead to unwanted signal reflections and distortions, affecting both amplitude and phase measurements. In our experiments, careful placement of the RTS and the use of controlled environments helped ~~to~~ minimize such distortions, leading to more reliable calibration outcomes. The ability to measure the transmit power of the radar provides another layer of validation, as the agreement between the measured and nominal transmit power confirms that the StXPol radar was tested in a multipath-free
540   environment. Because of the importance of conducting measurements without any ground reflections, we plan to conduct upcoming RTS calibrations on a drone platform, which not only improves the calibration accuracy but also enables precise antenna characterization (similar to Segales et al., 2024) and facilitates the experimental setup. Especially for lower frequency

radars like C- or S-band systems, finding clutter-free environments for conducting RTS tests becomes more demanding, since precision horn antennas with the same aperture size as at X-band frequencies exhibit a larger beamwidth and are hence more 545 prone to receiving ground reflections.

In conclusion, RTS provide an effective solution for weather radar calibration by enabling controlled and repeatable measurements of reflectivity, differential reflectivity, and Doppler velocity. Ensuring proper target placement and minimizing multi-path interference are crucial steps in achieving high calibration accuracy. Future improvements in RTS technology and experimental setup refinements will further enhance the precision and reliability of weather radar calibrations.

550 *Author contributions.* M. S. prepared the manuscript and developed the target simulator, Ph. S. calibrated the target simulator, conducted measurements and edited the manuscript. A. L. developed the target simulator and wrote Section 3. Ja. G. and H. C. operated StXpol, provided respective radar data and edited the manuscript. P. K. and Ji. G. operated CHILL and provided respective data. F. J. operated SPLASH and provided respective data. V. C. and A. B. supervised the experiments and edited the manuscript.

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